

# A SENSORLESS SLIDING MODE CONTROL BASED INDUCTION MOTOR DRIVE FOR INDUSTRIAL APPLICATION

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**Abstract**— Parameter identification plays an important role in speed estimation schemes. This paper presents a speed estimation scheme based on second-order sliding-mode super twisting algorithm (STA) and model reference adaptive system (MRAS) estimation theory, in which both variations of stator resistance and rotor resistance are deliberately treated. A stator current observer is designed based on the STA, which is utilized to take the place of the reference voltage model of the standard MRAS algorithm. The observer is insensitive to the variation of rotor resistance and perturbation when the states arrive at the sliding mode. Derivatives of rotor flux are obtained and designed as the state of MRAS, thus eliminating the integration. Furthermore, in order to improve the near-zero speed operation, a parallel adaptive identification of stator resistance is designed relying on derivatives of rotor flux and stator current. Compared with the first-order sliding-mode speed estimator, the proposed scheme makes full use of the auxiliary sliding-mode surface, thus alleviating the chattering behavior without increasing the complexity. The robustness and effectiveness of the proposed scheme have been validated experimentally.

**Keywords**— DC link, Induction Motor, Inverter, Inverse Park transformation, Model reference adaptive system, PI controller, Park Transformation, PWM, Rectifier, Sliding Mode Technique.

## 1. INTRODUCTION

With the invention of vector control technique the induction motor (IM) became popular for variable-speed drives and motion control. In indirect vector control of IM, flux and torque are decoupled under estimation of the slip speed with appropriate information of the rotor time constant. The accuracy of motor parameters, particularly, the rotor time constant plays an important role for the accuracy of the indirect vector method. To cope with that, recently, variable- structure controls (VSC), and in particular, sliding-mode control (SMC) system, have been applied for electric motor drive. The SMC-based drive system has many attractive features such as: 1) it is robust to parameter variations and model uncertainties and insensitive to external load disturbance; 2) it offers a fast dynamic response, and stable control system; 3) it can handle some nonlinear systems that are not stable by using linear controller; and, 4) it requires an easy hardware/software implementation. However, due to discontinuous nature, it has some limitations in electrical drives and shows high-frequency oscillations as chattering characteristics.

The chattering makes various undesirable effects such as current harmonics and torque pulsation. In recent years, the chattering issue has become the research focus of many scholars. Generally, introducing a thin boundary layer around the sliding surface can solve the chattering problem by interpolating a continuous function inside the boundary layer of switching surface. However, the slope of the continuous function is a compromise between control performance and chattering elimination. Also, asymptotic stability is not guaranteed and may cause a steady-state error.

## 2. OBJECTIVES OF THE THESIS

The objectives of the thesis are listed below:

- To reduce the overshoot of the DC link in existing system.
- To measure the speed without sensors.
- To use sliding mode technique to estimate speed.
- To acknowledge the efficient working of the existing system using this proposed system in the company.
- To design a model sufficient to prove the result.

### 3. BLOCK DIAGRAM OF EXISTING SYSTEM

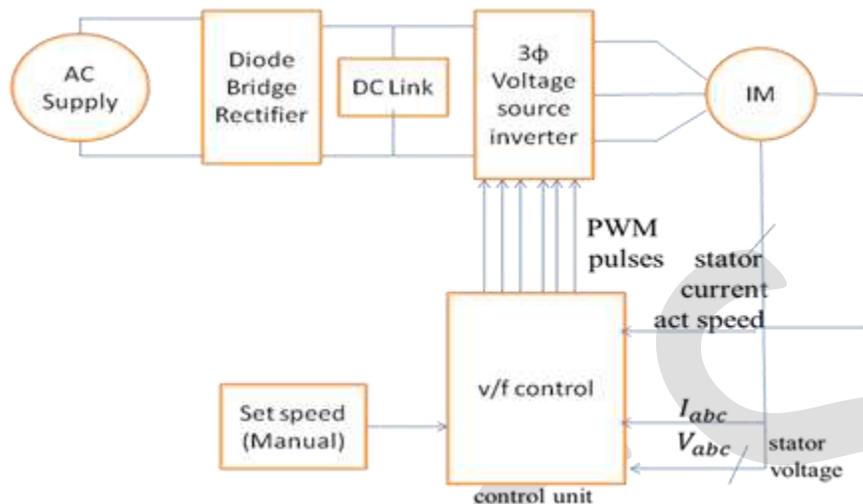


Fig 3.1: Block diagram of existing system.

The above block diagram shows the existing system, in this AC Supply given to diode bridge rectifier circuit. The input supply is converted to DC. The DC link circuit act as a mediator reducing the harmonics and over shoots. The DC link circuit output is input to three Phase voltage source inverter. The voltage source inverter drives the induction motor by converting by DC input to AC output. By using sensor we calculate actual speed, current, voltage. It is given to conventional PI controller and V/F controller and its compare the actual speed and set speed. The feedback is given to the PWM generator. The PWM generator is triggers the voltage source and thus the induction motor is controlled using direct input method.

#### 3.1 DRAWBACKS

- Using more sensors.
- Cost is high.

### 4. BLOCK DIAGRAM OF PROPOSED SYSTEM

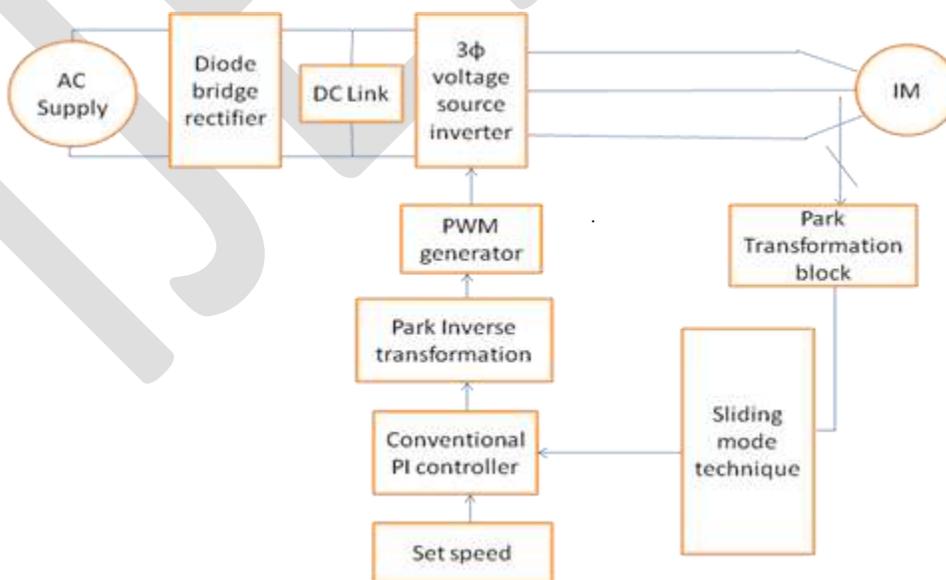


Fig 4.1 Block diagram of proposed system.

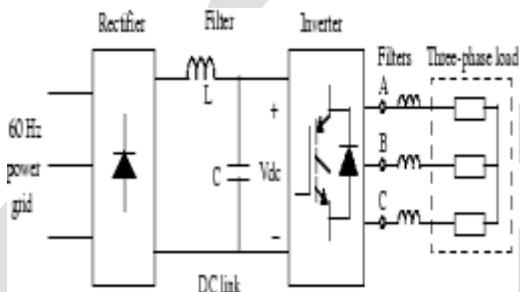
The above block diagram shows the proposed system, in this AC Supply given to diode bridge rectifier circuit. The input supply is converted to DC. The DC link circuit act as a mediator reducing the harmonics and over shoots. The DC link circuit output is input to three Phase voltage source inverter. The output current of voltage source inverter is given to park transformation. The park transformation converts the three phase current ( $I_a, I_b, I_c$ ) to two phase current ( $I_d, I_q$ ). From this current is taken as a reference and its used in sliding mode technique. In sliding mode technique we calculate the actual speed, magnetic flux, torque, rotor position. The output is given to control unit then it compare the actual speed and set speed. The feedback is given to inverse park transformation. The inverse park transformation is convert two phase current ( $I_d, I_q$ ) to three phase current ( $I_a, I_b, I_c$ ). The output current is given to the PWM generator and it triggers the voltage source and thus the induction motor is controlled using direct input method.

**4.1 DRAWBACKS**

The conventional H- Bridge inverter produces only two levels of output, it contains higher order of harmonics say third level . Say 50% of THD. The system consists of power electronics filters like inductive and capacitive for filtering purpose. This increases the cost and weight of the system. To overcome these drawback a new modified system is proposed .

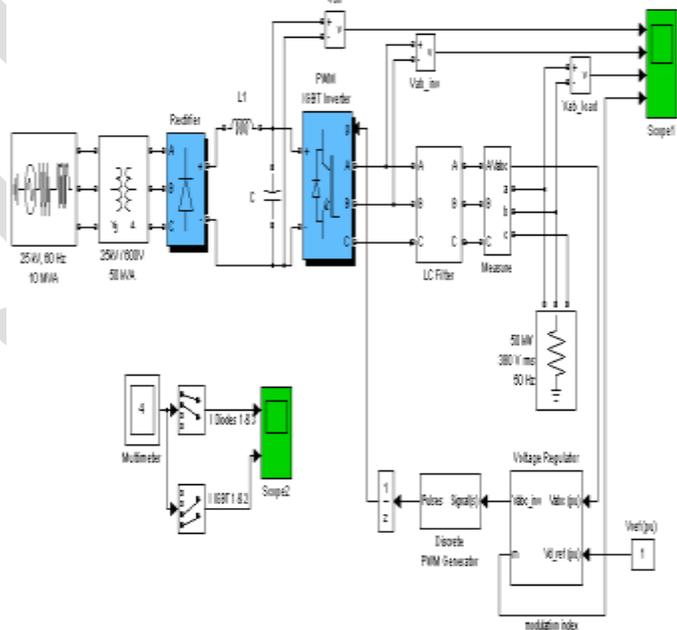
**5. UNIVERSAL BRIDGE**

The power bridges example illustrates the use of two Universal Bridge blocks in an ac/dc/ac converter consisting of a rectifier feeding an IGBT inverter through a DC link. The inverter is pulse-width modulated (PWM) to produce a three-phase 50 Hz sinusoidal voltage to the load. In this example the inverter chopping frequency is 4000 Hz.



**Fig 5.1** Example of universal bridge.

The IGBT inverter is controlled with a PI regulator in order to maintain a 1 pu voltage (380 Vrms, 50 Hz) at the load terminals. A Multimeter block is used to observe commutation of currents between diodes 1 and 3 in the diode bridge and between IGBT/Diodes switches 1 and 2 in the IGBT Bridge. Start simulation. After a transient period of approximately 40 ms, the system reaches a steady state. Observe voltage waveforms at DC bus, inverter output, and load on Scope1. The harmonics generated by the inverter around multiples of 2 kHz are filtered by the LC filter. As expected the peak value of the load voltage is 537 V (380 V RMS).

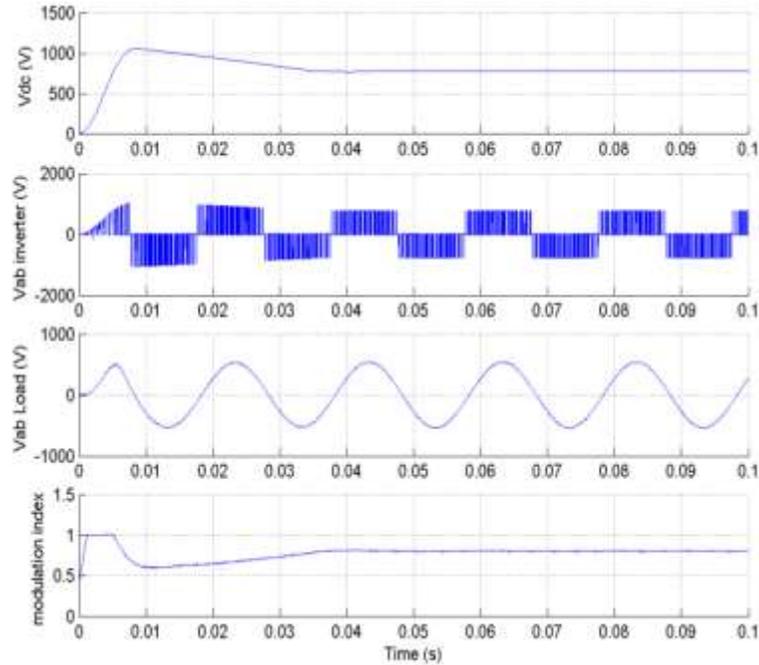


**Fig 5.1** Simulation diagram of universal bridge.

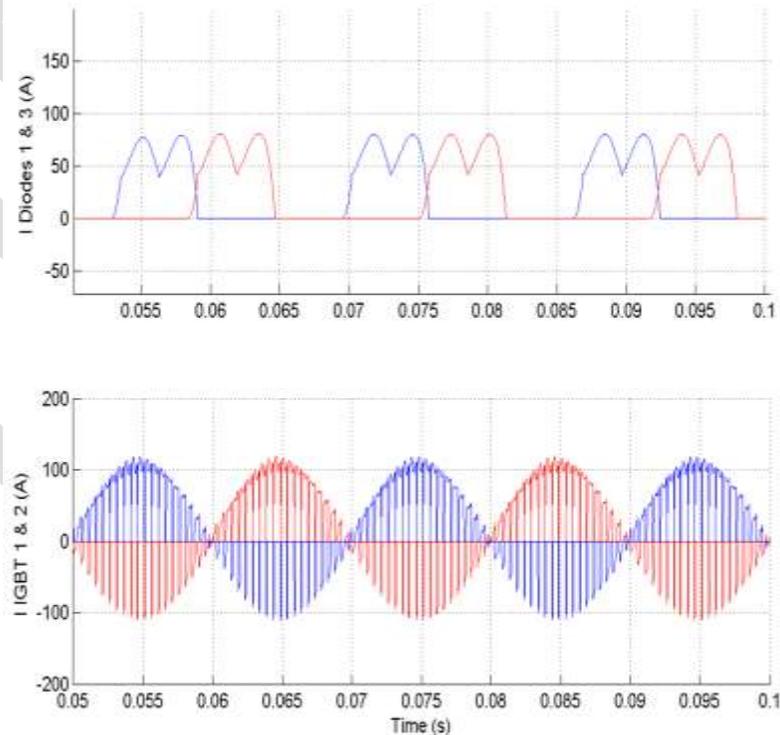
In steady state the mean value of the modulation index is  $m = 0.8$ , and the mean value of the DC voltage is 778 V. The fundamental component of 50 Hz voltage buried in the chopped inverter voltage is therefore

$$V_{ab} = 778 \text{ V} * 0.612 * 0.80 = 381 \text{ V RMS}$$

Observe diode currents on trace 1 of Scope2, showing commutation from diode 1 to diode 3. Also observe on trace 2 currents in switches 1 and 2 of the IGBT/Diode bridge (upper and lower switches connected to phase A). These two currents are complementary. A positive current indicates a current flowing in the IGBT, whereas a negative current indicates a current flowing in the antiparallel diode.



**Fig 5.2** Time(s) vs Modulation index, Vab load(v), Vab inverter(v), Vdc(v)



**Fig 5.3** Time(s) vs IGBT & Diode

## 6. INTRODUCTION TO PARK TRANSFORMATION

Perform Park transformation from three-phase (abc) reference frame to dq0 reference frame. The ransformations section of the Control and Measurements library contains the abc to dq0 block. This is an improved version of the abc\_to\_dq0 Transformation block. The new block features a mechanism that eliminates duplicate continuous and discrete versions of the same block by basing the block configuration on the simulation mode. If your legacy models contain the abc\_to\_dq0 Transformation block, they continue to work. However, for best performance, use the abc to dq0 block in your new models.

### 6.1 DESCRIPTION



Fig 6.1: Park transformation.

The abc\_to\_dq0 Transformation block computes the direct axis, quadratic axis, and zero sequence quantities in a two-axis rotating reference frame for a three-phase sinusoidal signal. The following transformation is used:  

$$V_d V_q V_0 = 23(V_a \sin(\omega t) + V_b \sin(\omega t - 2\pi/3) + V_c \sin(\omega t + 2\pi/3)) = 23(V_a \cos(\omega t) + V_b \cos(\omega t - 2\pi/3) + V_c \cos(\omega t + 2\pi/3)) = 13(V_a + V_b + V_c)$$
 where  $\omega$  = rotation speed (rad/s) of the rotating frame.

The transformation is the same for the case of a three-phase current; you simply replace the  $V_a, V_b, V_c, V_d, V_q,$  and  $V_0$  variables with the  $I_a, I_b, I_c, I_d, I_q,$  and  $I_0$  variables.

This transformation is commonly used in three-phase electric machine models, where it is known as a Park transformation. It allows you to eliminate time-varying inductances by referring the stator and rotor quantities to a fixed or rotating reference frame. In the case of a synchronous machine, the stator quantities are referred to the rotor.  $I_d$  and  $I_q$  represent the two DC currents flowing in the two equivalent rotor windings (d winding directly on the same axis as the field winding, and q winding on the quadratic axis), producing the same flux as the stator  $I_a, I_b,$  and  $I_c$  currents.

You can use this block in a control system to measure the positive-sequence component  $V_1$  of a set of three-phase voltages or currents. The  $V_d$  and  $V_q$  (or  $I_d$  and  $I_q$ ) then represent the rectangular coordinates of the positive-sequence component.

You can use the Math Function block and the Trigonometric Function block to obtain the modulus and angle of  $V_1$ :

$$\downarrow V_1 \downarrow \angle V_1 = G V_{2q} + V_{2d} = \text{atan2}(V_q/V_d)$$

This measurement system does not introduce any delay, but, unlike the Fourier analysis done in the Sequence Analyzer block, it is sensitive to harmonics and imbalances.

### 6.2 DIALOG BOX AND PARAMETERS

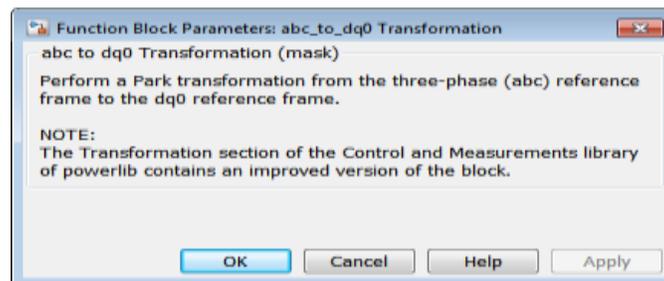


Fig 6.2: Dialog box and parameters.

### 6.3 INPUTS AND OUTPUTS

#### abc

Connect to the first input the vectorized sinusoidal phase signal to be converted [phase A phase B phase C].

#### sin\_cos

Connect to the second input a vectorized signal containing the  $[\sin(\omega t) \cos(\omega t)]$  values, where  $\omega$  is the rotation speed of the reference frame.

#### dq0

The output is a vectorized signal containing the three sequence components [d q o], in the same units as the abc input signal.

## 7. INTRODUCTION TO INVERSE PARK TRANSFORMATION

The Four Axis instance of this VI requires fixed size four elements arrays (one per axis) for all inputs, and returns fixed size four element array outputs. Calculates the Inverse Park Transform portion of the field-oriented control (FOC) commutation algorithm. The Inverse Park Transform modifies the flux,torque (d,q) rotating reference frame into a two phase orthogonal system (alpha,beta). The output is called the voltage vector. The data type you wire to any input determines the polymorphic instance to use.

### 7.1 Inverse Park Transformation (Single Axis)

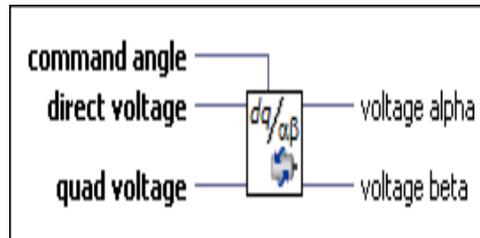


Fig 7.1 Single axis of inverse park transformation.

**command angle**—Specifies the calculated flux angle for the Park and Inverse Park transforms, in pi radian

**direct voltage**—Specifies the direct voltage value calculated by the flux/torque loop for use with the Inverse Park Transform.

**quad voltage**—Specifies the quad voltage value calculated by the flux/torque loop for use with the Inverse Park Transform.

**voltage alpha**—Specifies the alpha voltage calculated by the Inverse Park Transform for the Space Vector Modulation function.

**voltage beta**—Specifies the beta voltage calculated by the Inverse Park Transform for the Space Vector Modulation function.

### 7.2 Inverse Park Transformation (Four Axis)

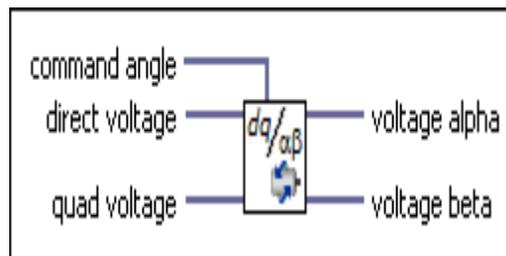


Fig 7.2 Four axis of inverse park transformation.

**command angle**—Specifies the calculated flux angle for the Park and Inverse Park transforms, in pi radians.

**direct voltage**—Specifies the direct voltage value calculated by the flux/torque loop for use with the Inverse Park Transform.

**quad voltage**—Specifies the quad voltage value calculated by the flux/torque loop for use with the Inverse Park Transform.

**voltage alpha**—Specifies the alpha voltage calculated by the Inverse Park Transform for the Space Vector Modulation function.

**voltage beta**—Specifies the beta voltage calculated by the Inverse Park Transform for the Space Vector Modulation function.

### 7.3 DETAILS

Use the Inverse Park Transform function to calculate the Inverse Park Transform portion of the field-oriented control (FOC) commutation algorithm, which modifies the flux, torque (d,q) rotating reference frame in a two phase orthogonal system (alpha, beta).

The Inverse Park Transform uses the following equations:

$$v_{\alpha} = v_d \cos \theta - v_q \sin \theta$$

$$v_{\beta} = v_d \sin \theta + v_q \cos \theta$$

Where

$v_{\alpha}$  is the alpha voltage,

$v_d$  is the direct voltage,

$v_q$  is the quad voltage,

$v_{\beta}$  is the beta voltage, and

$\theta$  is the angle of rotation for the transformed reference frame.

The following figure shows the NI Soft Motion FOC commutation algorithm block diagram, and the location of the Inverse Park Transform within it.

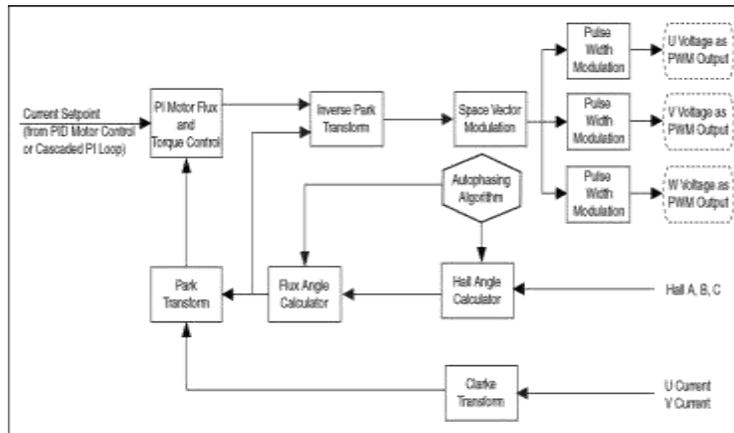


Fig 7.3 Block diagram NI Soft Motion FOC commutation algorithm.

### 7.4 FIXED-POINT DETAILS

The Motor Control VIs use fixed-point values when possible. When you wire fixed-point values to Motor Control VIs, the VIs usually return values that do not lose any bits of word length. However, if the operation creates a value that exceeds the maximum word length that LabVIEW accepts, overflow or rounding conditions can occur. LabVIEW accepts a maximum word length of 64 bits. Refer to Using the Fixed-Point Data Type in the FPGA Module help for information about how fixed-point numbers might impact timing.

## 8. SLIDING MODE TECHNIQUE

### 8.1 STATOR CURRENT:



The park transformation converts the three phase current to two phase ( $I_{sd}$ ,  $I_{sq}$ )

$I_{abc}$  = Stator current

$I_{sd}$  = Stator direct current

$I_{sq}$  = Stator quadrature current

## 8.2 STATOR VOLTAGE:



The park transformation converts the three phase current to two phase ( $V_{sd}, V_{sq}$ )

$V_{abc}$  = Stator voltage

$V_{sd}$  = Stator direct voltage

$V_{sq}$  = Stator quadrature voltage

### STATOR FLUX :

$$\varphi_{sd} = \int V_d - R_s \cdot I_{sd} \quad (1)$$

$$\varphi_{sq} = \int V_q - R_s \cdot I_{sq} \quad (2)$$

Where,

$$I_{sd} = \frac{2}{3} \left( I_a - \frac{1}{2} I_b - \frac{1}{2} I_c \right) \quad (3)$$

$$I_{sq} = -\frac{2}{3} \left( -(\sqrt{3}/2) I_b + (\sqrt{3}/2) I_c \right) \quad (4)$$

$\varphi_{sd}$  = Direct stator flux

$\varphi_{sq}$  = Quadrature stator flux

$V_d$  = Direct voltage

$V_q$  = Quadrature voltage

$R_s$  = Stator Resistance

### MAGNITUDE OF STATOR FLUX :

$$\text{Magnitude of stator flux} = \sqrt{(\varphi_{sd}^2 + \varphi_{sq}^2)} \quad (5)$$

### ROTOR POSITION:

$$\theta = \tan^{-1} \left( \frac{\varphi_{sq}}{\varphi_{sd}} \right) \quad (6)$$

Where,

$\theta$  = Rotor position.

### TORQUE ESTIMATOR:

$$T_e = (3/2) p (\varphi_{sd} * I_{sq} - \varphi_{sq} * I_{sd}) \quad (7)$$

Where,

$P$  – no of poles

$$\text{Slip} = T_e * (R_r / 2) \quad (8)$$

Where,

$T_e$  = Estimated torque

$R_r$  = Rotor resistance

### ELECTRICAL SPEED:

$$\text{Electrical speed} = (\text{speed of field-slip}) / \text{square of rotor flux} \quad (9)$$

$$\text{Speed of rotor field} = \varphi_{rd} * \varphi_{r\beta} - \varphi_{rq} * \varphi_{r\alpha} \quad (10)$$

### ROTOR FLUX :

$$\varphi_{rd} = (L_M / L_R) \varphi_{sd} \quad (11)$$

$$\varphi_{rq} = (L_M / L_R) \varphi_{sq} \quad (12)$$

### MECHANICAL SPEED:

$$\omega_m = (1/2) * \text{Electrical speed.} \quad (13)$$

Where,

$\omega_m$  = Mechanical speed

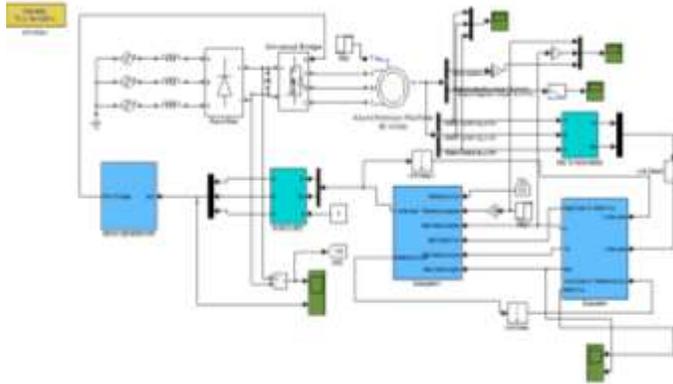
In sliding mode technique we calculate the actual speed, magnetic flux, torque, rotor position. The output is given to control unit then it compare the actual speed and set speed

## 9. SIMULATIONS AND RESULTS

The detailed description about the result of the proposed system with the help of MATLAB and the results of the simulated system is drawn here.

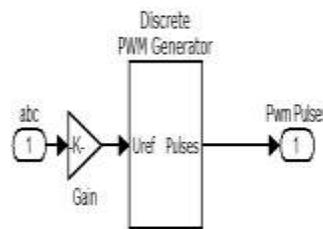
### 9.1 SIMULATION DIAGRAM

The simulation diagram of proposed system is shown below.



**Fig 9.1:** Simulation diagram of the proposed system.

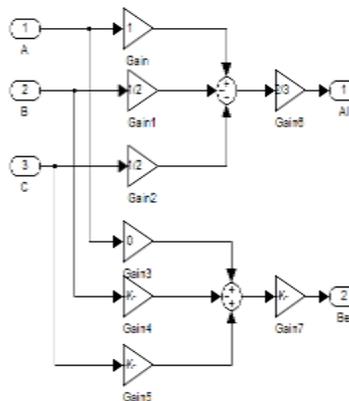
### 9.2 TRIGGER CIRCUIT SPWM GENERATOR



**Fig 9.2:** Circuit diagram of SPWM generator.

The output from the inverse park transformation is fed into selector bus and the gain is added with it. The output from the gain is fed into SPWM generator the PWM pulses are produced.

### 9.3 TRIGGER CIRCUIT PARK TRANSFORMATION



**Fig 9.3:** Circuit Diagram of A1-Be to ABC.

The stator current is fed into the gain and is summed up in the summing point and three phases converted into two phase stator current.

### 9.4 TRIGGER CIRCUIT INVERSEPARK TRANSFORMATION

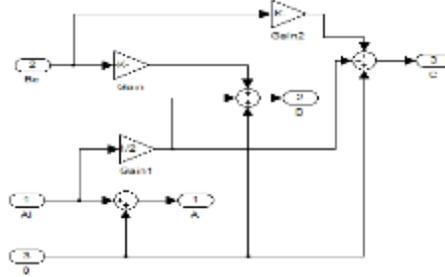


Fig 9.4: Circuit diagram of inverse park transformation.

In this circuit by adding gains and summing point with references the two phase again converted into three phase.

### 9.5 TRIGGER CIRCUIT PI CONTRLLER

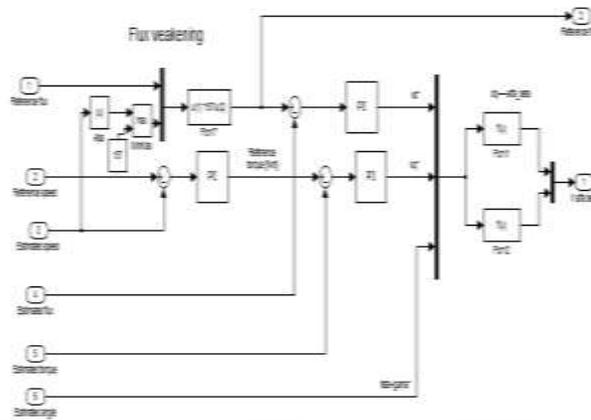


Fig 9.5 : Circuit diagram of PI controller.

The reference speed, estimated speed ,reference flux, estimated flux, estimated angle ,estimated torque are given to control unit.It compares the actual speed and set speed and its given to the inverse park transformation.

### 9.6 TRIGGER CIRCUIT SLIDING MODE

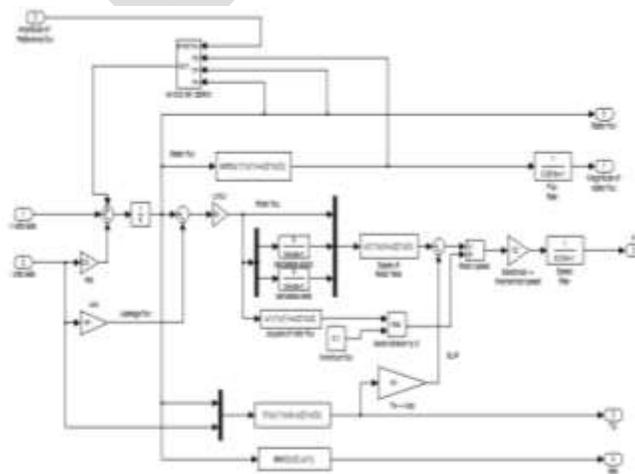


Fig 9.6: circuit diagram of sliding mode control.

The flux and voltage are taken as reference and the feedback current is fed into gain then it is given to derivative alpha and beta. Then the output is given to the speed of rotor flux and it is converted as electrical to mechanical speed. The final estimated speed is obtained.

## 9.7 OUTPUT OF SIMULATION MODEL

### 9.7.1 SPEED CHARACTERISTICS

X axis: Time in seconds  
Y axis: speed in rpm

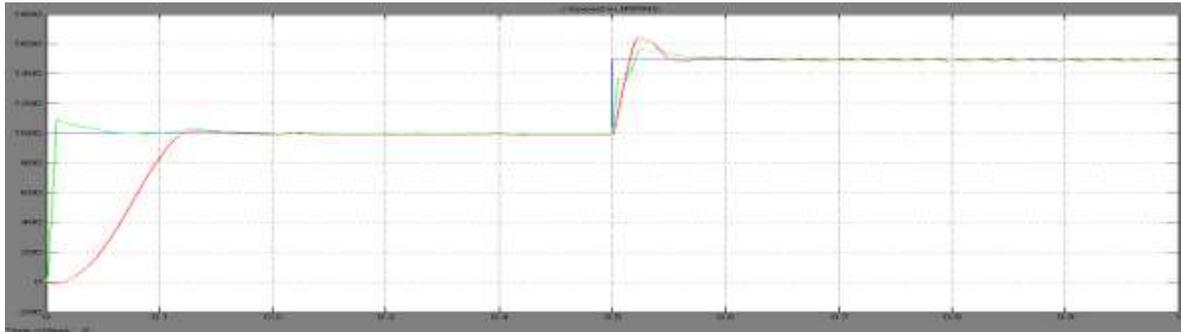


Fig 9.7: Time Vs Speed characteristics.

In the above graph shows the characteristics of Speed.

- The blue colour line shows the estimated speed.
- The pink colour line shows the reference speed.
- The green colour line shows the actual speed.

### 9.7.2 VOLTAGE CHARACTERISTICS

X axis : Time in seconds  
Y axis : Direct current voltage ( $V_{dc}$ )

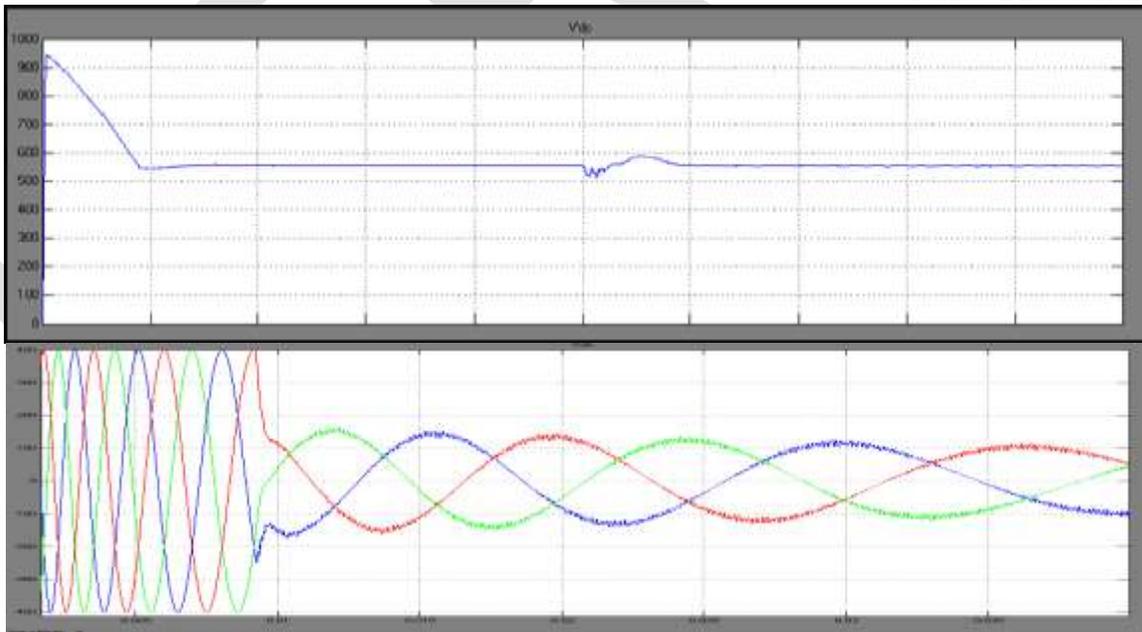


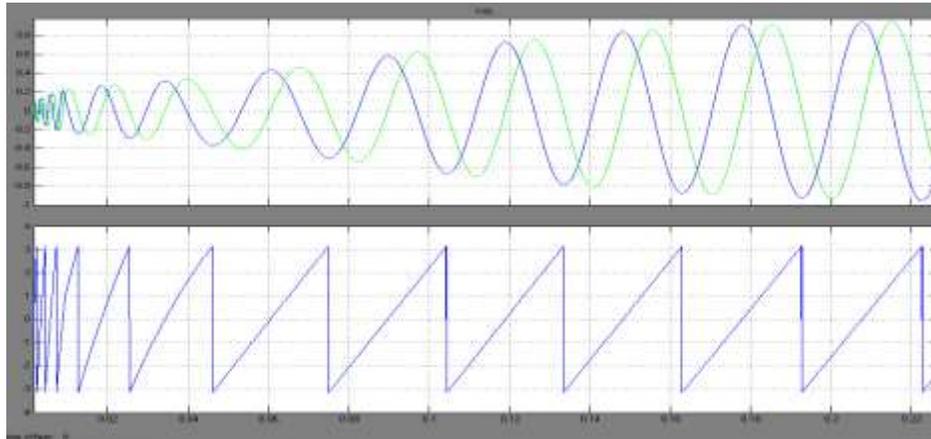
Fig 9.8(a) and (b) : Time Vs voltage ( $V_{dc}$ ).

In the above graph shows the characteristics of voltage.

- The blue colour line shows the estimated speed.
- The pink colour line shows the reference speed.
- The green colour line shows the actual speed.

### 9.7.3 TORQUE CHARACTERISTICS

X axis : Time in seconds  
Y axis : Direct current voltage ( $V_{dc}$ )



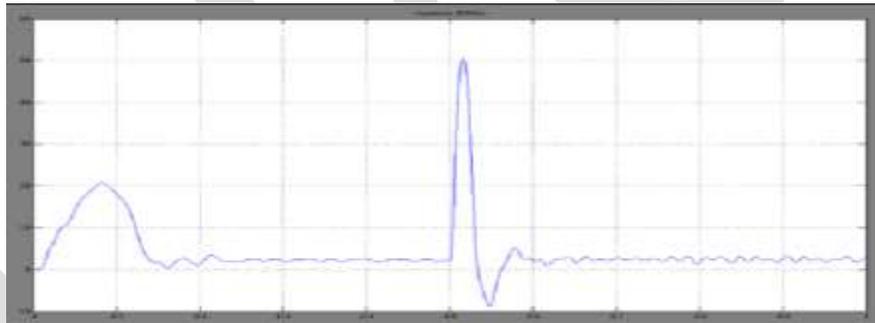
**Fig 9.9 (a) and (b) : Time Vs voltage ( $V_{dc}$ ).**

In the above graph shows the characteristics of torque.

- The blue colour line shows the estimated speed.
- The pink colour line shows the reference speed.
- The green colour line shows the actual speed.

### 9.7.4 STATOR FLUX CHARACTERISTICS

X axis : Time in seconds  
Y axis : Speed in rpm



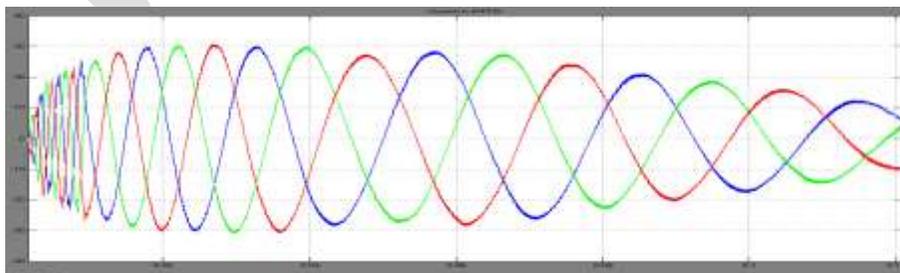
**Fig 9.10 : Time Vs Speed**

In the above graph shows the characteristics of stator flux.

- The blue colour line shows the estimated speed.
- The pink colour line shows the reference speed.
- The green colour line shows the actual speed.

### 9.7.5 STATOR CURRENT CHARACTERISTICS

X axis : Time in seconds  
Y axis : Speed in rpm



**Fig 9.11 : Time Vs Speed.**

In the above graph shows the characteristics of stator current.

- The blue colour line shows the estimated speed.
- The pink colour line shows the reference speed.
- The green colour line shows the actual speed.

## 10. CONCLUSION

This paper presents a modified speed-sensorless control scheme based on second-order sliding-mode STA and MRAS estimation theory. The estimation scheme has been obtained by combining a second-order sliding-mode current observer with a parallel speed and stator resistance estimator based on rotor flux-based MRAS. Both the error in instantaneous phase position and the error in amplitudes are used respectively for speed estimation and  $R_s$  identification, thus overcoming the problems of  $R_s$  variation, particularly for low-speed operation.

The STA-based observer is utilized to take the place of the reference voltage model of the standard MRAS. Derivatives of rotor flux are obtained and designed as the state of MRAS, thus eliminating the integration. Moreover, by making full use of auxiliary surfaces, the observations are insensitive to rotor parameter perturbation with the alleviation of chattering behavior at the same time. The proposed scheme is insignificantly more complex than its counterpart with speed estimation only, so it is easy to implement in the already existing MRAS-based speed estimator. However, since the scheme is designed based on the mathematical model of IM, its observability is generally lost at zero magnetic field frequency. Machine state observability can be improved by additional stator voltage change injection, which is considered to be the further work.

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